

EECS 247

Analog-Digital Interface Integrated Circuits

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Lecture 1: Introduction

Instructor's Technical Background

- Ph.D., EECS department -UC Berkeley 1985, advisor Prof. P.R. Gray
 - Thesis topic: Continuous-time CMOS high-frequency filters
- Industrial background
 - 11 years at ATT & Bell Laboratories, N.J., in the R&D area as a circuit designer
 - Circuits for wireline communications: CODECs, ISDN, and DSL including ADCs (nyquist rate & over-sampled), DACs, filters, VCOs
 - Circuits intended for wireless applications
 - Fiber-optics circuits
 - 3 years at Philips Semiconductors, Sunnyvale, CA
 - Managed a group in the RF IC department- developed ICs for CDMA & analog cell phones
 - 3 years @ Broadcom Corp. – Director of Analog/RF ICs in San Jose, CA.
 - Projects: Gigabit-Ethernet, TV tuners, and DSL circuitry
 - Currently consultant for IC design
- Teaching experience
 - Has taught/co-taught EE247 @ UCB since 2003
 - Instructor for short courses offered by MEAD Electronics
 - Adjunct Prof. @ Rutgers Univ., N.J. : Taught a graduate level IC course

Administrative

- Course web page:
<http://inst.eecs.berkeley.edu/~EE247>
 - Course notes will be uploaded on the course website prior to each class
 - Homeworks & due dates are posted on the course website
 - Please visit course website often for announcements
- Lectures are webcast mainly for the benefit of students @ UCSC
<http://webcast.berkeley.edu/courses>
 - Please try to attend the classes live to benefit from direct interactions
 - Make sure you use the provided microphones when asking questions or commenting in class

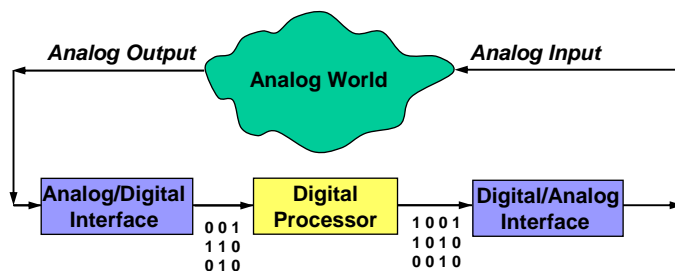
Office Hours & Grading

- Office hours:
 - Tues./Thurs. 2:30-3:30pm @ 563 Cory Hall (unless otherwise announced in the class)
 - Extra office hours by appointment
 - Feel free to discuss issues via email:
haidehk@eecs.berkeley.edu
- Course grading:
 - Homework/project 50%
 - Midterm 20% (tentative date: Oct. 18)
 - Final 30%

Prerequisites & CAD Tools

- Prereqs.
 - Basic course in signal processing (Laplace and z-transform, discrete Fourier transform) i.e. EE120
 - Fundamental circuit concepts i.e. EE105 and EE140
- CAD Tools:
 - HSPICE or Spectre
 - Matlab

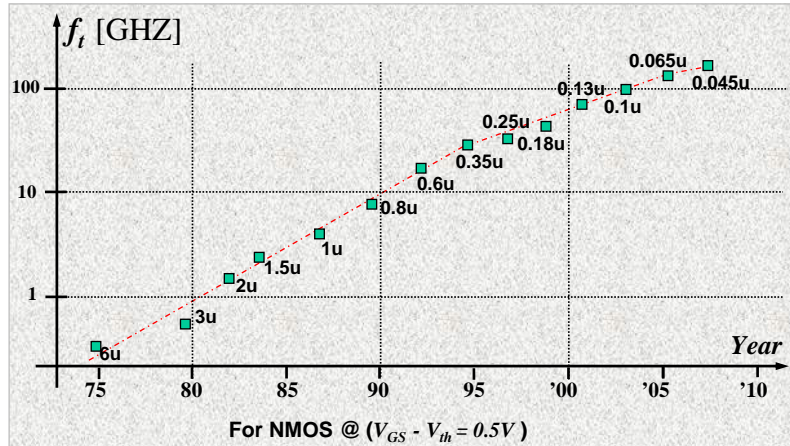
Analog-Digital Interface Circuitry



- Naturally occurring signals are analog
- To process signals in the digital domain
 - ∴ Need Analog/Digital & Digital/Analog interface circuitry

Question: Why not process the signal with analog circuits only & thus eliminate need for A/D & D/A?

CMOS Technology Evolution versus Time



*Ref: Paul R. Gray UCB EE290 course '95

International Technology Roadmap for Semiconductors,

<http://public.itrs.net>

CMOS Device Evolution Progression from 1975 to 2005

- Feature sizes ~X1/100
- Cut-off frequency f_t ~X300
- Minimum size device area ~ $1/L^2$
- Number of interconnect layers ~X8

Impact of CMOS Scaling on Digital Signal Processing

Direct beneficiary of VLSI technology down scaling

- Digital circuits deal with “0” & “1” signal levels only
 - Not sensitive to “analog” noise
- Si Area/function reduced drastically due to
 - Shrinking of feature sizes
 - Multi metal levels for interconnections (currently >8 metal level v.s. only 1 in the 1970s)
- Enhanced functionality & flexibility
- Amenable to automated design & test
- “Arbitrary” precision
- Provides inexpensive storage capability

Analog Signal Processing Characteristics

- Sensitive to “analog” noise
- Has not fully benefited from technology down scaling:
 - Supply voltages scale down accordingly
 - Reduced voltage swings → more challenging analog design
 - Reduced voltage swings requires lowering of the circuit noise to keep a constant dynamic range
 - Higher power dissipation and chip area
- Not amenable to automated design
- Extra precision comes at a high price
- Rapid progress in DSP has imposed higher demands on analog/digital interface circuitry
 - **Plenty of room for innovations!**

Cost/Function Comparison DSP & Analog

- Digital circuitry: Fully benefited from CMOS device scaling
 - Cost/function decreases by ~29% each year
 - ❖ Cost/function X1/30 in 10 years*
 - Analog circuitry: Not fully benefited from CMOS scaling
 - Device scaling mandates drop in supply voltages → threaten analog feasibility
 - ❖ Cost/function for analog ckt almost constant or increase
- Rapid shift of function implementation from processing in analog domain to digital & hence increased need for A/D & D/A interface circuitry

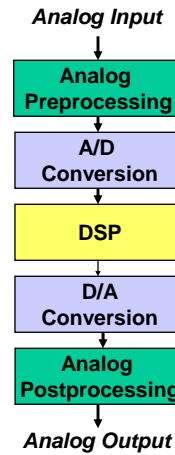
*Ref: International Technology Roadmap for Semiconductors, <http://public.itrs.net>

Digitally Assisted Analog Circuitry

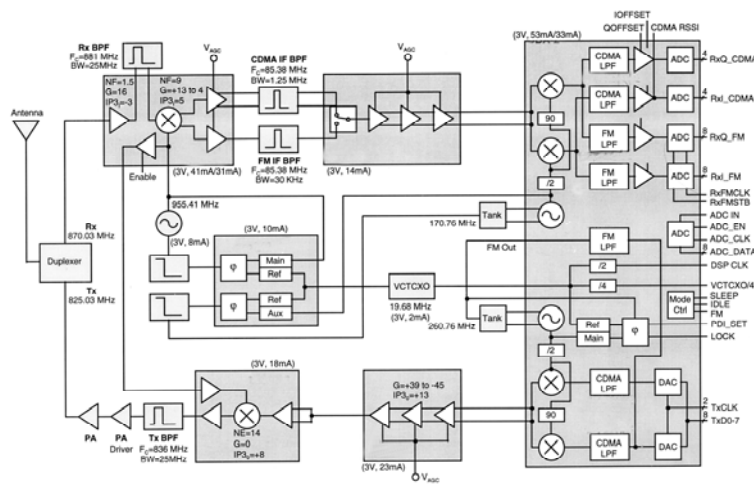
- Analog design has indeed benefited from the availability of inexpensive on-chip digital capabilities
- Examples:
 - Compensating/calibrating ADC & DAC inaccuracies
 - Automatic frequency tuning of filters & VCOs
 - DC offset compensation

Example: Digital Audio

- Goal-Lossless archival and transmission of audio signals
- Circuit functions:
 - Preprocessing
 - Amplification
 - Anti-alias filtering
 - A/D Conversion
 - Resolution→16Bits
 - DSP
 - Storage
 - Processing (e.g. recognition)
 - D/A Conversion
 - Postprocessing
 - Smoothing filter
 - Variable gain amplification



Example: Dual Mode CDMA (IS95)& Analog Cellular Phone RF & Baseband



Example: Typical Dual Mode Cell Phone



Contains in integrated form:

- 4 RX filters
 - 3 or 4 TX filters
 - 4 RX ADCs
 - 2 TX DACs
 - 3 Auxiliary ADCs
 - 8 Auxiliary DACs
- } Dual Standard, I/Q
- } Audio, Tx/Rx power control, Battery charge control, display, ...

Total: Filters → 8

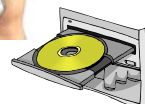
ADCs → 7

DACs → 12

Areas Utilizing Analog/Digital Interface Circuitry

• Communications

- Wireline communications
 - Telephone related (DSL, ISDN, CODEC)
 - Television circuitry (Cable modems, TV tuners...)
 - Ethernet (Gigabit, 10/100Base T...)
- Wireless
 - Cellular telephone (CDMA, Analog, GSM...)
 - Wireless LAN (Blue tooth, 802.11a/b/g....)
 - Radio (analog & digital), Television
 - Personal Data Assistants



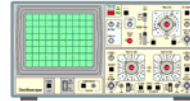
• Computing & Control

- Storage media (disk drives, digital tape)
- Imagers & displays

Areas Utilizing Analog/Digital Interface Circuitry

- **Instrumentation**

- Electronic test equipment & manufacturing environment ATEs
- Semiconductor test equipment
- Physical sensors & actuators
- Medical equipment



- **Consumer Electronics**

- Audio (CD, DAT, MP3)
- Automotive control, appliances, toys



UCB Analog Courses EECS 247 - 240 - 242

- EECS 240
 - Transistor level, building blocks such as opamps, buffers, comparator....
 - Device and circuit fundamentals
 - CAD Tools → SPICE
- EECS 247
 - Filters, ADCs, DACs, some system level
 - Signal processing fundamentals
 - Macro-models, large systems, some transistor level, constraints such as finite gain, supply voltage, noise, dynamic range considered
 - CAD Tools → Matlab, SPICE
- EECS 242
 - RF amplification, mixing
 - Oscillators
 - Exotic technology devices
 - Nonlinear circuits

Material Covered in EE247

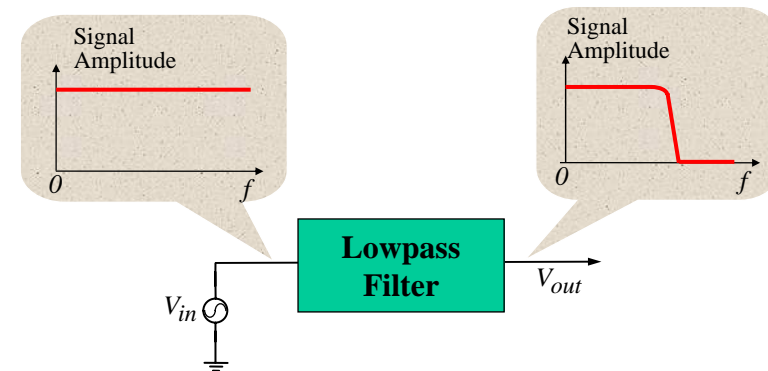
- Filters
 - Continuous-time filters
 - Biquads & ladder type filters
 - Opamp-RC, Opamp-MOSFET-C, gm-C filters
 - Automatic frequency tuning techniques
 - Switched capacitor (SC) filters
- Data Converters
 - D/A converter architectures
 - A/D converter
 - Nyquist rate ADC- Flash, Pipeline ADCs,....
 - Oversampled converters
 - Self-calibration techniques
- Systems utilizing analog/digital interfaces
 - Wireline communication systems- ISDN, XDSL...
 - Wireless communication systems- Wireless LAN, Cellular telephone,...
 - Disk drive electronics
 - Fiber-optics systems

Books (on reserve @ Eng. Library) (NOT required to be purchased),

- Filters
 - A. Williams and F. Taylor, *Electronic Filter Design Handbook*, 3rd edition, McGraw-Hill, 1995.
 - W. Heinlein & W. Holmes, "Active Filters for Integrated Circuits", Prentice Hall Int., Inc. Chap. 8, 1974. Good reference for signal flowgraph techniques
 - A. Zverev, *Handbook of Filter Synthesis*, Wiley, 1967.
A classic; focus is on passive ladder filters. Tables for implementing ladder filters (replaces a CAD tool).
 - Data Converters
 - R. van de Plassche, *Integrated Analog-to-Digital and Digital-to-Analog Converters*, 2nd edition, Kluwer, 2003.
 - B. Razavi, *Data Conversion System Design*, IEEE Press, 1995.
 - S. Norsworthy et al (eds), *Delta-Sigma Data Converters*, IEEE Press, 1997.
 - General
 - Gray, Hurst, Lewis, Meyer, *Analysis & Design of Analog Integrated Circuits*, Wiley 2001.
 - Johns, Martin, *Analog Integrated Circuit Design*, Wiley 1997.
- ❖ Note: a list of relevant IEEE publications is posted on the course website. Some will be noted as mandatory reading and the rest optional

Introduction to Filters

- Filtering → Provide frequency selectivity and/or phase shaping
 - Oldest & most common type of signal processing



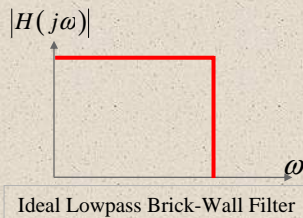
Introduction to Filters

- Typical filter applications:
 - Extraction of desired signal from many (radio, TV, cell phone, ADSL.....)
 - Separating signal and noise
 - Anti-aliasing
 - Phase equalization
 - Amplifier bandwidth limitations

Ideal versus Practical Filters Example: Lowpass Filter

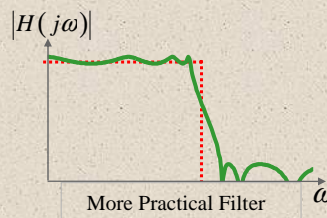
- Ideal filter

- Brick-wall characteristics
- Flat magnitude response in the passband
- Infinite level of rejection of out-of-band signals

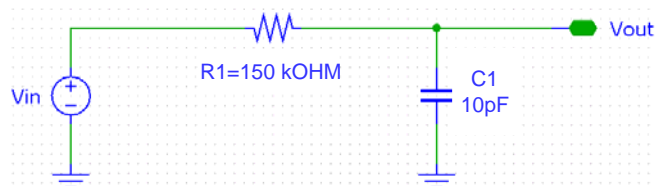


- Practical filter

- Ripple in passband magnitude response
- Limited rejection of out-of-band signals



Simplest Filter First-Order RC Filter (LPF1)



Steady-state frequency response:

$$H(s) = \frac{V_{out}(s)}{V_{in}(s)} = \frac{1}{1 + \frac{s}{\omega_0}}$$

with
$$\omega_0 = \frac{1}{RC} = 2\pi \times 100 \text{ kHz}$$

S-Plane Poles and Zeros

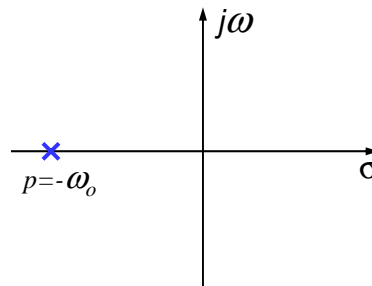
$$H(s) = \frac{1}{1 + \frac{s}{\omega_o}}$$

Pole: $p = -\omega_o$

Zero: $z \rightarrow \infty$

$$|H(s)| = \left| \frac{1}{1 + j \frac{\omega}{\omega_o}} \right| = \frac{1}{\sqrt{1 + \frac{\omega^2}{\omega_o^2}}}$$

s-plane (pzmap):



Filter Frequency Response Bode Plot

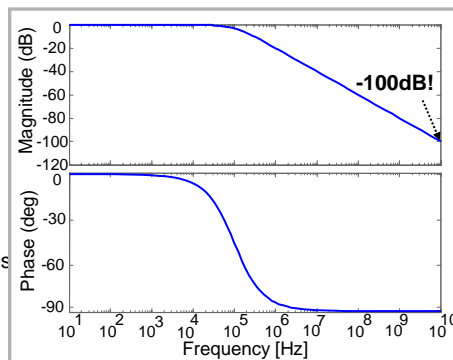
$$|H(s = j\omega)|_{\omega=0} = 1$$

$$|H(s = j\omega)|_{\omega=\omega_o} = 1/\sqrt{2}$$

$$|H(s = j\omega)|_{\omega \rightarrow \infty} = 0$$

Asymptotes:

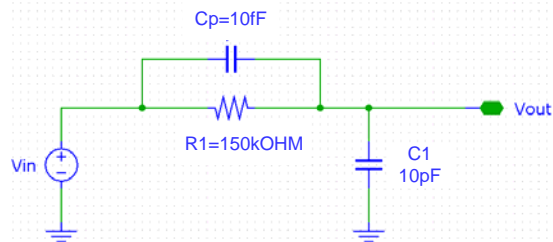
- 20dB/dec magnitude rolloff
- 90degrees phase shift per 2 decades



Question:

can we really get 100dB attenuation at 10GHz?

First-Order Low-Pass RC Filter Including Parasitics (LPF2)



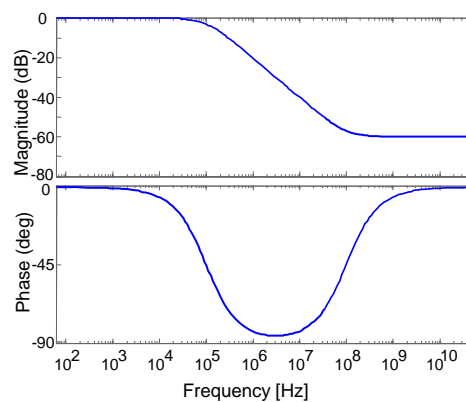
$$H(s) = \frac{1 + sRC_P}{1 + sR(C + C_P)}$$

$$\text{Pole: } p = -\frac{1}{R(C + C_P)} \approx -\frac{1}{RC}$$

$$\text{Zero: } z = -\frac{1}{RC_P}$$

Filter Frequency Response

$$\begin{aligned} |H(j\omega)|_{\omega=0} &= 1 \\ |H(j\omega)|_{\omega \rightarrow \infty} &= \frac{C_P}{C + C_P} \\ &\approx \frac{C_P}{C} \\ &= 10^{-3} \\ &= -60\text{dB} \end{aligned}$$



- Beware of other parasitics not included in this model ...

Dynamic Range & Electronic Noise

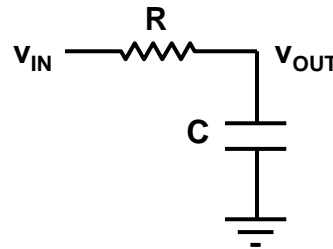
- Dynamic range is defined as the ratio of maximum possible signal handled by a circuit to the minimum useful signal
 - Maximum signal handling capability usually determined by maximum possible voltage swings which in turn is a function of supply voltage & circuit non-linearity
 - Minimum signal handling capability is normally determined by electronic noise
 - Amplifier noise due to device thermal and flicker noise
 - Resistor thermal noise
- Dynamic range in analog ckts has direct implications for power dissipation

Analog Dynamic Range

- Once the poles and zeroes of the analog filter transfer function are defined then special attention must be paid to the actual implementation
- Of the infinitely many ways to build a filter with a given transfer function, **each of those combinations result in a different level of output noise!**
- As an example noise and dynamic range for the 1st order lowpass filter will be derived

First Order Filter Noise

- Capacitors are noiseless
- Resistors have thermal noise
 - This noise is uniformly distributed from dc to infinity
 - Frequency-independent noise is called “white noise”



Resistor Noise

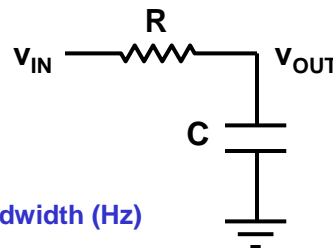
- Resistor noise characteristics
 - A mean value of zero
 - A mean-squared value

$$\overline{v_n^2} = 4k_B T_r R \Delta f$$

Labels for the equation:

- Volts² (points to $\overline{v_n^2}$)
- ohms (points to R)
- absolute temperature (°K) (points to T_r)
- measurement bandwidth (Hz) (points to Δf)

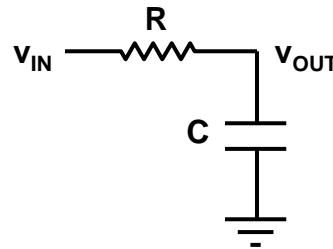
Boltzmann's constant = $1.38e-23$ J/°K



Resistor Noise

- Theoretically, resistor rms noise voltage in a 10Hz band centered at 1kHz is the same as resistor rms noise in a 10Hz band centered at 1GHz
- Resistor noise spectral density, N_0 , is the rms noise per $\sqrt{\text{Hz}}$ of bandwidth:

$$N_0 = \sqrt{\frac{v_n^2}{\Delta f}} = \sqrt{4k_B T_r R}$$



Resistor Noise

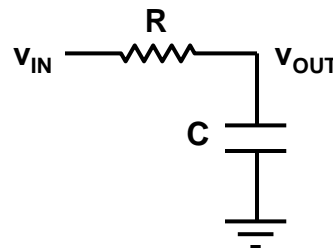
Good numbers to memorize:

- N_0 for a **1k Ω** resistor at room temperature is **4nV/ $\sqrt{\text{Hz}}$**
- Scaling R,
 - A 10M Ω resistor gives 400nV/ $\sqrt{\text{Hz}}$
 - A 50 Ω resistor gives 0.9nV/ $\sqrt{\text{Hz}}$
- Or, remember

$$k_B T_r = 4 \times 10^{-21} \text{ J} \quad (T_r = 17^\circ \text{C})$$

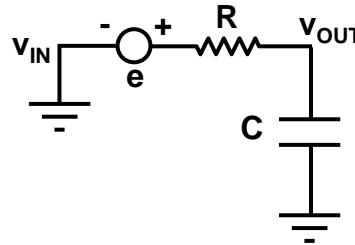
- Or, remember

$$k_B T_r / q = 26 \text{ mV} \quad (q = 1.6 \times 10^{-19} \text{ C})$$



First Order Filter Noise

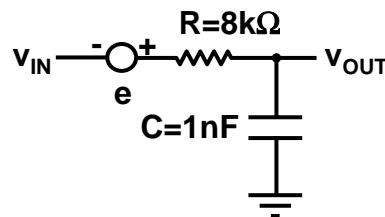
- To derive noise @ the output node:
 - Short circuit the input to ground.
 - Resistor noise gives the filter a non-zero output when $v_{IN}=0$
 - In this simple example, both the input signal and the resistor noise obviously have the same transfer functions to the output
 - Since noise has random phase, we can use any polarity convention for a noise source (but we have to use it consistently)



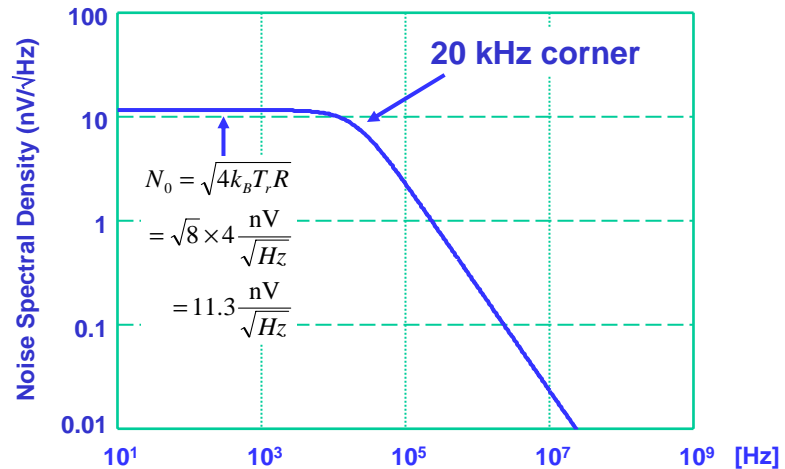
First Order Filter Noise

- What is the thermal noise of this RC filter?
- Let's ask SPICE!
Netlist:

```
*Noise from RC LPF
vin vin 0 ac 1V
r1 vin vout 8kOhm
c1 vout 0 1nF
.ac dec 100 10Hz 1GHz
.noise V(vout) vin
.end
```



LPF1 Output Noise Spectral Density



Total Noise

- Total noise is what the display on a volt-meter connected to v_o would show!
- Total noise is found by integrating the noise power spectral density within the frequency band of interest
- Note that noise is integrated in the mean-squared domain, because noise in a bandwidth df around frequency f_1 is uncorrelated with noise in a bandwidth df around frequency f_2
 - Powers of uncorrelated random variables add
 - Squared transfer functions appear in the mean-squared integral

$$\overline{v_o^2} = \int_{f_1}^{f_2} \overline{v_n^2} |H(j\omega)|^2 df$$

$$\overline{v_o^2} = \int_0^{\infty} 4k_B T R |H(2\pi jf)|^2 df$$

*Ref: "Analysis & Design of Analog Integrated Circuits", Gray, Hurst, Lewis, Meyer- Chapter 11

Total Noise

$$\begin{aligned}\overline{v_o^2} &= \int_0^{\infty} 4k_B T R |H(2\pi j f)|^2 df \\ &= \int_0^{\infty} 4k_B T R \left| \frac{1}{1 + 2\pi j f R C} \right|^2 df\end{aligned}$$

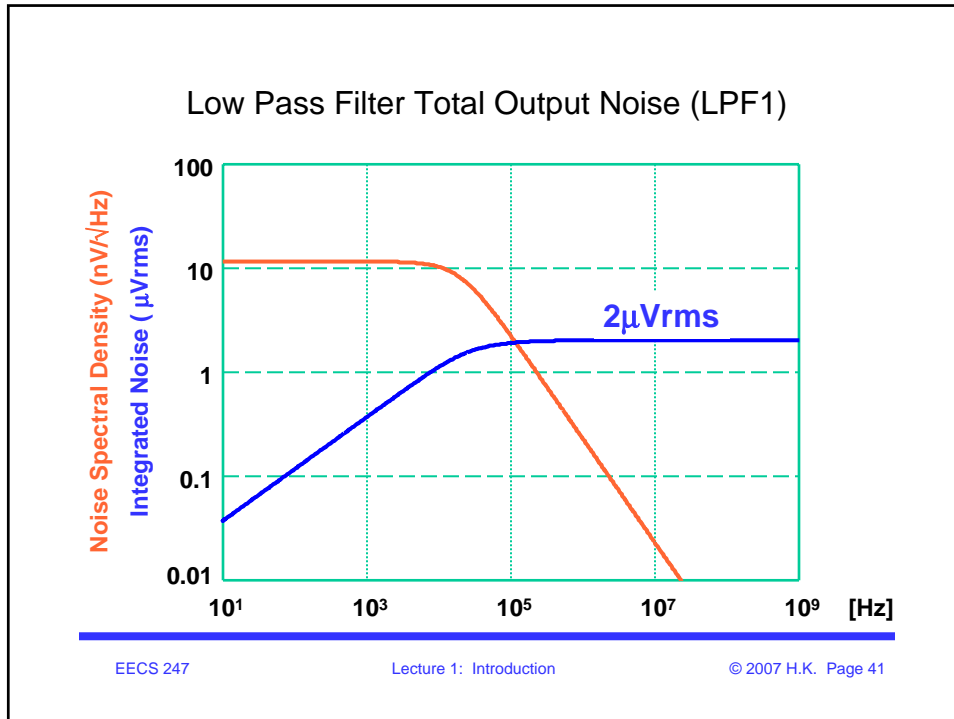
$$\rightarrow \boxed{\overline{v_o^2} = \frac{k_B T}{C}}$$

- This interesting and somewhat counter intuitive result means that even though resistors are the components generating the noise, total noise is determined by noiseless capacitors!
- For a given capacitance, as resistance goes up, the increase in noise density is balanced by a decrease in noise bandwidth

kT/C Noise

- kT/C noise is a fundamental analog circuit limitation
- The rms noise voltage of the simplest possible (first order) filter is $(k_B T/C)^{1/2}$
- For 1pF capacitor, $(k_B T/C)^{1/2} = 64 \mu\text{V-rms}$ (at 298°K)
- 1000pF gives 2 $\mu\text{V-rms}$
- The noise of a more complex & higher order filter is given by:
 $(\alpha \times k_B T/C)^{1/2}$

where α depends on implementation and features such as filter order

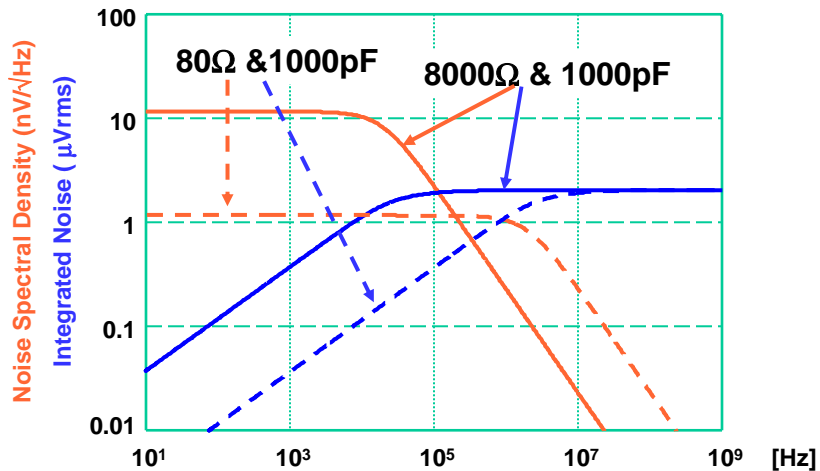


LPF1 Output Noise

- Note that the integrated noise essentially stops growing above 100kHz for this 20kHz lowpass filter
- Beware of faulty intuition which might tempt you to believe that an 80Ω , 1000pF filter has lower integrated noise compared to our 8000Ω , 1000pF filter...

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LPF1 Output Noise



Analog Circuit Dynamic Range

- Maximum voltage swing for analog circuits -assuming no inductors are used!- can at most be equal to power supply voltage V_{DD} (normally is smaller)
- Assuming a sinusoid signal $\rightarrow V_{\max}(rms) = \frac{1}{\sqrt{2}} \frac{V_{DD}}{2}$

- Noise for a filter $\rightarrow V_n(rms) = \sqrt{\alpha \frac{k_B T}{C}}$

$$D.R. = \frac{V_{\max}(rms)}{V_n(rms)} = \frac{V_{DD} \sqrt{C}}{\sqrt{8\alpha k_B T}} \quad [V/V]$$

\rightarrow Dynamic range in dB is:

$$= 20 \log_{10} \left(V_{DD} \sqrt{\frac{C}{\alpha}} \right) + 75 \quad [\text{dB}] \quad \text{with } C \text{ in [pF]}$$

Analog Circuit Dynamic Range

- For integrated circuits built in modern CMOS processes, $V_{DD} < 1.5V$ and $C < 100pF$ ($\alpha = 1$)
 - $D.R. < 98 dB$
- For PC board circuits built with “old-fashioned” $30V$ opamps and discrete capacitors of $< 100nF$
 - $D.R. < 140dB$
 - A $42dB$ advantage!

Dynamic Range versus Number of Bits

- Number of bits and dB are related:
$$D.R. = (1.76 + 6.02N) \text{ [dB]} \quad N \rightarrow \text{number of bits}$$
 - see “quantization noise”, later in the course
- Hence

98 dB	\rightarrow	16 Bits
140 dB	\rightarrow	23 Bits

Dynamic Range versus Power Dissipation

- Each extra bit corresponds to 6dB extra dynamic range
- Increasing dynamic range by one bit \rightarrow 6dB less noise \rightarrow decrease in noise power by 4x!
- This translates into 4x larger capacitors
- To keep speed constant (speed prop G_m/C): G_m must increase 4x
- Power is proportional to G_m (for fixed supply and V_{dsat})

In analog circuits with performance limited by thermal noise,

1 extra bit costs 4x power

E.g. 16Bit ADC at 200mW \rightarrow 17Bit ADC at 800mW

Do not overdesign the dynamic range of analog circuits!

Noise Summary

- Thermal noise is a fundamental property of (electronic) circuits
- In filters, noise is closely related to
 - Capacitor size
- In higher order filters, noise is a function of C, filter order, Q, and depends on implementation
- Operational amplifiers used in active filters can contribute significant levels of extra noise to overall filter noise
- Reducing noise in most analog circuits is costly in terms of power dissipation and chip area